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Algebraic codes for Slepian-Wolf code design

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Abstract—Practical constructions of lossless distributed source codes (for the Slepian-Wolf problem) have been the subject of much investigation in the past decade. In particular, near-capacity achieving code designs based on LDPC codes have been presented for the case of two binary sources, with a binary-symmetric correlation. However, constructing practical codes for the case of non-binary sources with arbitrary correlation remains by and large open. From a practical perspective it is also interesting to consider coding schemes whose performance remains robust to uncertainties in the joint distribution of the sources.

In this work we propose the usage of Reed-Solomon (RS) codes for the asymmetric version of this problem. We show that algebraic soft-decision decoding of RS codes can be used effectively under certain correlation structures. In addition, RS codes offer natural rate adaptivity and performance that remains constant across a family of correlation structures with the same conditional entropy. The performance of RS codes is compared with dedicated and rate adaptive multistage LDPC codes (Varodayan et al. '06), where each LDPC code is used to compress the individual bit planes. Our simulations show that in classical Slepian-Wolf scenario, RS codes outperform both dedicated and rate-adaptive LDPC codes under q -ary symmetric correlation, and are better than rate-adaptive LDPC codes in the case of sparse correlation models, where the conditional distribution of the sources has only a few dominant entries. In a feedback scenario, the performance of RS codes is comparable with both designs of LDPC codes. Our simulations also demonstrate that the performance of RS codes in the presence of inaccuracies in the joint distribution of the sources is much better as compared to multistage LDPC codes.

I. INTRODUCTION

We consider the problem of practical code design for the Slepian-Wolf problem. Following the work of [1] that established the equivalence between the Slepian-Wolf problem and channel coding, a lot of research work has addressed this problem (see [2] and its references). However, by and large most of the work considers the case of two binary sources that are related by an additive error. In this paper, we propose a coding scheme for nonbinary sources using Reed-Solomon codes that works under more general correlation models than an additive error model. One previously proposed approach for compressing two nonbinary sources is to use several LDPC codes, each for a bit level of the binary image [3] along with multistage decoding. It requires the knowledge of the joint distribution and the conditional distributions of the binary sources that corresponding to the bit levels. It also requires the design of multiple LDPC codes, multiple LDPC decodings at the terminal and may suffer from error propagation. The multistage LDPC approach breaks down the symbol level correlation to bit level correlations. When the correlation is essentially at the symbol level, multistage LDPC

may not be the most suitable approach. In this paper we evaluate the performance of RS codes and multistage LDPC codes. We note that very few simulation results of multistage LDPC codes for Slepian-Wolf problem on large alphabet sizes have appeared in previous work. Turbo code-based design of nonbinary SWC was proposed in [4] but only field size of eight was considered. The work of [5] proposed algebraic codes for SWC using list decoding. Our algorithm uses soft decoding and has better performance. In addition, we provide simulations and comparisons with multistage LDPC codes.

In this paper, two scenarios are considered in our simulation. One is the classical Slepian-Wolf scenario, where there is no feedback from the decoder to the encoder. In the other scenario, there is feedback from the decoder to the encoder that tells the encoder whether the decoding is successful. If the decoding fails, the encoder will send more syndrome symbols. In this paper, we consider two designs of multistage LDPC codes [3], (i) Dedicated codes for each bit source. The degree distributions of the codes are optimized for AWGN channels and the codes are generated by PEG algorithm [6]. These codes do not offer rate adaptivity. (ii) The rate adaptive codes designed in [7]. The rate adaptivity in Slepian-Wolf problem requires us to adapt the transmission rate by adapting the syndrome length, rather than code length. If a low transmission rate is not enough to decode the source, more syndrome symbols are transmitted to the decoder and together with previously received syndrome, the decoder attempts to decode. RS codes offer natural rate-adaptivity by definition. Rate adaptive codes are useful in the feedback scenario. Our simulations show that in the classical Slepian-Wolf coding scenario, under q -ary symmetric correlation models, RS codes outperform both designs of multistage LDPC codes. Under sparse correlation models, RS codes perform better than rate adaptive LDPC codes when the correlation resembles q -ary symmetric models. In the feedback scenario, the performance of rate-adaptive LDPC codes and RS codes are comparable under q -ary symmetric channels but under sparse correlation model, rate-adaptive LDPC codes perform better than RS codes. Moreover, when the correlation given to the decoder is slightly different from the true correlation model, RS codes suffer little but multistage LDPC codes suffer significantly.

This paper is organized as follows. The preliminaries about RS codes and the Koetter-Vardy decoding algorithm [8] are given in Section II. The RS code-based asymmetric SWC schemes are described in Section III and the performance comparisons with a single LDPC codes are presented in Section IV. In Section V and Section VI the performance comparisons of RS codes and multistage LDPC codes under two scenarios are presented respectively. Section VII concludes the paper.

II. PRELIMINARIES

Let F_q be a finite field and q be a power of two. A (n, k) RS code can be defined by its parity check matrix $H_{ij} = (\alpha^i)^{j-1}, i = 1, \dots, n-k, j = 1, \dots, n$, where α is a primitive element of F_q and $n = q - 1$. The code $\mathcal{C}_{RS} = \{\mathbf{c} \in F_q^n : H_{RS}\mathbf{c} = 0\}$. Suppose H_1, H_2 are the parity check matrices of two RS codes with rates $k_1/n, k_2/n$ respectively and $k_1 \geq k_2$, by definition, H_1 is a submatrix of H_2 . As we shall see later, this allows rate adaptivity for distributed source coding. An equivalent definition of an RS code is given in terms of polynomial evaluation. Given a message vector \mathbf{m} of length k , the encoded codeword is obtained by evaluating the message polynomial $f_{\mathbf{m}}(\mathcal{X})$ (of degree $k-1$) at n points $\{1, \alpha, \alpha^2, \dots, \alpha^{n-1}\}$. One only needs to specify the code parameters n and k when designing codes.

Consider a channel coding scenario. A codeword $\mathbf{c} \in \mathcal{C}_{RS}$ is transmitted and the channel output is \mathbf{r} . Let $\gamma_1, \dots, \gamma_q$ be a fixed ordering of the elements from F_q . The receiver computes the q -by- n reliability matrix $\Pi = \{\pi_{ij} = P(c_j = \gamma_i | r_j)\}$ based on the information from the channel. The Koetter-Vardy soft decoding algorithm [8] first computes a multiplicity matrix M from Π . The simplest choice is $M = \lfloor \lambda \Pi \rfloor$, where λ is a positive real number. Next, it constructs a bivariate polynomial $Q_M(\mathcal{X}, \mathcal{Y})$ with minimal weighted degree that passes through every point $(\alpha^{j-1}, \gamma_i), m_{ij}$ times. These algebraic constraints can be given by $C(M)$ linear constraints, where $C(M) = \frac{1}{2} \sum_{i=1}^q \sum_{j=1}^q m_{ij}(m_{ij} + 1)$ is called the cost of M . Finally it identifies all the factors of $Q_M(\mathcal{X}, \mathcal{Y})$ of type $\mathcal{Y} - f(\mathcal{X})$, where $f(\mathcal{X})$ has degree no more than $k-1$. Among these, it picks the candidate with the highest likelihood based on the channel pmf. Note that the row index of M can also be given by an element from the F_q , i.e., $m_j(\beta) = m_{ij}$ if $\beta = \gamma_i$. The score of a vector \mathbf{v} with respect to a multiplicity matrix M is defined to be $S_M(\mathbf{v}) = \sum_{j=1}^n m_j(v_j)$. If the entries in M corresponding to the transmitted codeword \mathbf{c} have large values, then \mathbf{c} has high score w.r.t. M . It has been shown [8] that as long as the score of a codeword $S_M(\mathbf{c}) \geq \Delta_{1,k-1}(C(M))$, \mathbf{c} will appear on the candidate list, i.e., the decoding is successful. $\Delta_{1,k-1}(C(M))$ is defined in [8] and depends on k and $C(M)$ (increases with them).

III. RS CODES FOR ASYMMETRIC SWC

Consider an asymmetric SWC scenario where source X is available at the terminal. If an RS code is used, the encoding for \mathbf{y} is its syndrome $\mathbf{s} = H\mathbf{y}$. The decoder needs to find the most probable $\hat{\mathbf{y}}$ that belongs to the coset with syndrome \mathbf{s} . Upon obtaining \mathbf{x} , the decoder finds the reliability matrix $\Pi = \{\pi_{ij} = P(Y_j = \gamma_i | X_j = x_j)\}$ based on the joint distribution. Then, use the multiplicity algorithms to find a multiplicity matrix M . The simplest choice is $M = \lfloor \lambda \Pi \rfloor$. If the RS code is powerful enough to correct the errors introduced by the correlation channel, the score $S_M(\mathbf{y})$ should satisfy the score condition. We want to obtain \mathbf{y} from the matrix M by interpolation and factorization. Note that \mathbf{y} is not a codeword but belongs to a coset with syndrome \mathbf{s} . This requires us to modify the KV algorithm appropriately. An approach to modify Guruswami and Sudan's hard decision decoding algorithm [9] to syndrome decoding was proposed

in [10] and [5] independently. Our approach is motivated by them. Find a \mathbf{z} belonging to the coset with syndrome \mathbf{s} . This can be done by letting any k entries in \mathbf{z} to be zero and solve $H\mathbf{z} = \mathbf{s}$. The uniqueness of the solution is guaranteed by the MDS property of the RS code. Construct a shifted multiplicity matrix M' from M according to \mathbf{z} , where $m'_j(\gamma_i) = m_j(\gamma_i + z_j)$, or, equivalently, $m'_j(\gamma_i + z_j) = m_j(\gamma_i)$, for $1 \leq i \leq q, 1 \leq j \leq n$. Interpolate the $Q_{M'}(\mathcal{X}, \mathcal{Y})$ according to M' as in KV algorithm and find the list of candidate codewords $\mathcal{L}_{\mathbf{c}}$ by factorization. Adding \mathbf{z} to each candidate codeword we obtain the set of candidates $\mathcal{L}_{\mathbf{y}}$ for \mathbf{y} . **Claim:** $\mathbf{y} \in \mathcal{L}_{\mathbf{y}}$ if $H\mathbf{y} = \mathbf{s}$ and $S_M(\mathbf{y}) \geq \Delta_{1,k-1}(C(M))$.

Proof: The interpolation and factorization ensure that if a codeword \mathbf{c} is such that $S_{M'}(\mathbf{c}) \geq \Delta_{1,k-1}(C(M'))$, $\mathbf{c} \in \mathcal{L}_{\mathbf{c}}$. Note that each column of M' is just a permutation of the corresponding column of M , so $C(M) = C(M')$ and $\Delta_{1,k-1}(C(M')) = \Delta_{1,k-1}(C(M))$. If a vector \mathbf{y} satisfies $H\mathbf{y} = \mathbf{s}$ and $S_M(\mathbf{y}) \geq \Delta_{1,k-1}(C(M))$, $\mathbf{y} + \mathbf{z}$ is a codeword and $S_{M'}(\mathbf{y} + \mathbf{z}) = \sum_{j=1}^n m'_j(y_j + z_j) = \sum_{j=1}^n m_j(y_j) = S_M(\mathbf{y}) \geq \Delta_{1,k-1}(C(M'))$, thus $\mathbf{y} + \mathbf{z} \in \mathcal{L}_{\mathbf{c}}$. So $\mathbf{y} \in \mathcal{L}_{\mathbf{y}}$. ■

Next, the decoder performs ML decoding on $\mathcal{L}_{\mathbf{y}}$ based on Π . It is shown in the simulations that this step is almost always correct. Thus, if \mathbf{y} satisfies the score condition, the decoding is successful (with very high probability). The performance of the algorithm depends on the multiplicity assignment, during which the correlation between the sources is exploited.

Remark: 1) The soft information we used is the conditional pdf $P(Y|X)$. It does not require the correlation model to be additive. So it is suitable for more general correlation models.

2) RS codes enable rate adaptivity easily because of the structure of the parity check matrix. Suppose a syndrome $H_1\mathbf{y}$ is available at the decoder but the decoding fails. The terminal wants to know $H_2\mathbf{y}$, where H_2 has $(n-k_2)$ rows and $k_1 \geq k_2$. We can transmit additional inner products of \mathbf{y} and newly added rows in H_2 and together with the syndrome received previously, the decoder obtains the syndrome $H_2\mathbf{y}$. Then the decoder works for a code with lower code rate.

IV. COMPARISON WITH A SINGLE LDPC CODE

RS codes are Maximum Distance Separable (MDS) codes. However, it is well known that RS codes are not capacity-achieving over probabilistic channels such as the BSC and the q -ary symmetric channel. On the other hand, LDPC codes are capacity-achieving under binary symmetric channels. It is expected and observed in simulation that for *binary* correlated sources, LDPC codes have better performance. However, we expect that RS codes could be a better fit for sources over large alphabets, at least for the channels that resemble deterministic channels, e.g., q -ary symmetric channels.

One simple way to use LDPC codes in nonbinary Slepian-Wolf coding is to use a single LDPC code to encode the binary image of the nonbinary symbols. Consider a correlation model for sources X and Y expressed as $X = Y + E$, where $X, Y, E \in F_{512}$ such that E is independent of X and the agreement probability $P_a = P(E = 0) = 1 - p_e, P(E = \gamma) = p_e/(q-1)$ for nonzero $\gamma \in F_{512}$. X and Y are uniformly distributed. This is called q -ary symmetric correlation model. RS codes are defined over F_{512} with length 511. The LDPC

codes for comparison have length 4599 and a maximum variable node degree of 30 and were generated using the PEG algorithm [6]. For a given source pair, we use one LDPC code and encode for the binary image of the source outputs and the initial bit level LLR for belief propagation decoding is found by appropriate marginalization. We used three different code rates. For each code, we increase P_a (decrease $H(Y|X)$) until the frame error rate was less than 10^{-3} and recorded the corresponding $H(Y|X)$ as the maximum $H(Y|X)$ that allows us to perform near error-free compression. The results are available in Table I. We observe that LDPC has larger

TABLE I
COMPARISON OF RS CODES AND LDPC CODES

k/n	Tx Rate (bits/sym)	RS max $H(Y X)$	LDPC max $H(Y X)$
0.2	7.2	5.3175	3.7855
0.3	6.3	4.3770	3.3740
0.5	4.5	2.8474	1.7271

gap between the $H(Y|X)$ and the actual transmission rate than RS codes. As expected, RS codes also have a gap to the optimal rate. We also run the unique decoding algorithm for RS codes (Berlekamp-Massey algorithm) and observe that the performance is better than LDPC codes but worse than KVA.

V. COMPARISON WITH MULTISTAGE LDPC CODES: CLASSICAL SLEPIAN-WOLF SCENARIO

A. Multistage LDPC codes

Multistage LDPC codes have been proposed for Slepian-Wolf coding for nonbinary alphabets in prior work [3]. To compress a source with alphabet size q , we can view it as $r = \log_2 q$ binary sources. Suppose X is known at the terminal and the source Y is represented as bit sources $Y_{b_1}, Y_{b_2}, \dots, Y_{b_r}$. The source transmits the syndromes of each bit source sequence, $s_k = H_k y_{b_k}, k = 1, 2, \dots, r$, where H_k is the parity check matrix of a LDPC code. At the decoder, the side information X is given, and to decode the k th bit source, the previous decoded bit sources can also be used as side information, based on which the initial LLR is computed. The decoding requires us to decode r LDPC codes.

The design of optimized LDPC codes for our problem requires us to consider the individual bit level channels and the distribution of the input LLRs at each bit level. This is a somewhat complicated task and is part of ongoing work. Here we use the following two designs for comparison.

1) *Dedicated LDPC codes*: We optimize the degree distribution using density evolution for AWGN channel¹. Then, the code of length 512 is designed by PEG algorithm². We design LDPC codes with rates 0.02, 0.04, 0.06, \dots , 0.90, a total of 45 codes. These codes are designed separately and do not provide rate adaptivity.

¹As explained before, ideally we should run density evolution for the actual bit level channel broken down from the symbol level correlation channel. This is part of ongoing work. In addition, we require a large number of codes in order to match the required rates at the different bit levels. Since AWGN optimized LDPC codes are known to have very good performance in related channels such as the BSC, we chose to work with them for the comparison.

²We need to choose a block length for each LDPC code so that the comparison with the RS code of length 255 (8-bit symbols) is fair. We chose a length of 512, that is approximately 2×255 . With higher LDPC block lengths, one can expect better performance.

2) *Rate-adaptive LDPC codes*: Designed in [7], these irregular LDPC codes have length 6336 and the code rate can be chosen among $\{0/66, 1/66, \dots, 64/66\}$. The structure of their parity check matrices allow us to use them in a rate-adaptive manner. Note that these codes have a very high block length.

B. Simulation Setting

We consider classical SWC scenario. Given a correlation model, we gradually increase the transmission rate until the frame error rate is less than 10^{-3} . The decoder attempts decoding only once. For LDPC codes, a frame is in error if one of the decodings is in error. When we adjust the transmission rate, we adjust the rate of the LDPC codes for each bit source, so that the FER for each bit source are of the same order. To get the FER $< 10^{-3}$ at nonbinary symbol level, the FERs at the bit level are roughly 10^{-4} . For each rate configuration, we simulate until the number of error frame is at least 100. The maximum iteration time of the belief propagation algorithm is 100. For RS codes, the field size $q = 256$ and the length $n = 255$. $\lambda = 100.99$ in the multiplicity assignment. We increase the transmission rate until the FER $< 10^{-3}$. The decoder attempts decoding only once.

C. q -ary symmetric correlation model

The simulation results for q -ary ($q = 256$) symmetric correlation model under different agreement probabilities are given in Fig. 1 (solid lines). The gaps between actual transmission rates and $H(Y|X)$ are presented. Larger gap indicates worse performance. We observe that under q -ary symmetric correlation models RS codes outperform both types of LDPC codes. This coincides with our intuition since the q -ary symmetric is favorable for RS codes. Note that RS codes performs better when the agreement probability P_a is very high or very low. For low P_a , a RS code with low rate is used and it is observed before [8] that the Koetter-Vardy algorithm performs better for low rate codes. When P_a is very low, for multistage LDPC codes, only a portion of bit sources can be compressed, several bit sources need to be transmitted at rate one.

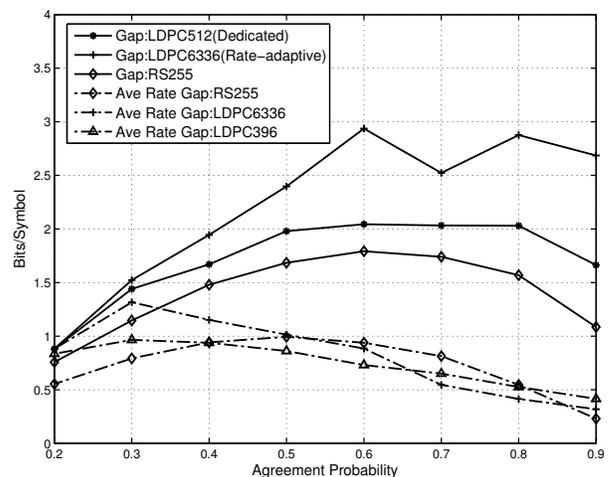


Fig. 1. The gap between the transmission rate and $H(Y|X)$ for multistage LDPC and RS codes under q -ary symmetric models. Solid line represents classical SWC scenario and the dash-dot line represents feedback scenario.

D. Sparse correlation model

When the correlation model becomes more general, RS codes do not always outperform LDPC codes. Under the correlation model where each column of the conditional probability matrix $P(Y|X = j)$ contains a few dominant terms, it is possible that RS codes still perform well. We call such kind of correlation models to be sparse. We shall compare the performance of multistage LDPC codes and RS codes under sparse correlation models defined as follows.

Definition 1: We say a conditional pdf $P(Y|X)$ is (S, ϵ) -sparse if for every $j = 1, \dots, q$, $P(Y = i|X = j), i = 1, \dots, q$ have S entries that are greater than ϵ .

We are mostly interested in (S, ϵ) -sparse conditional pdf $P(Y|X)$ with $S \ll q$ and $\epsilon \ll 1$, i.e., for each j , $P(Y = i|X = j)$ has few dominant entries. For those entries with probability mass less than ϵ , we assume that the probabilities are the same. When X is uniformly distributed, the joint pdf is also sparse and we call such a correlation model, a sparse correlation model. For a (S, ϵ) -sparse conditional pdf $P(Y = i|X = j)$, denote the vector of the S dominant entries by $D(j)$. We assume that the dominant entries are the same for all j and denote them by D . For example, for a q -ary symmetric correlation model with $q = 256$ and $P_a = 0.8$, $D = [0.8]$ and it is $(1, 10^{-3})$ -sparse. For a fixed D , there are a lot of choices of the locations of the dominant entries. We consider the following dominant entry patterns.

The dominant entries can be put in the *diagonal form*, a generalization of q -ary symmetric correlation model. The largest entries are on the diagonal of the conditional pdf matrix and other entries are put around them. For example, consider a joint pdf with $(3, 10^{-3})$ -sparse conditional distribution and $D = [0.1 \ 0.6 \ 0.1]$. When it is placed in the diagonal form, $P(Y = j|X = j) = 0.6$ for all j , $P(Y = j - 1|X = j) = 0.1$ for all j except $j = 1$, $P(Y = j + 1|X = j) = 0.1$ for all j except $j = 256$ and $P(Y = 256|X = 1) = P(Y = 1|X = 256) = 0.1$. All other entries are $(1 - 0.1 - 0.6 - 0.1)/253 < 10^{-3}$. The dominant entries in a conditional pdf is said to be in the *random form* if D is uniformly randomly placed in the column $P(Y|X = j)$. Note that this randomness only appear in the determination of the pdf and it will be fixed during all transmissions. This correlation model is a model $Y = X + E$ where E depends on X (data dependent model). Note that different placements of probability masses in the columns of conditional distribution do not change the conditional entropy $H(Y|X)$, and do not affect the performance of KV algorithm for RS codes. But the performance of multistage LDPC codes changes when the placement of probability masses changes. In simulations, multistage LDPC codes performs better under diagonal form conditional distribution than the random form.

Note that a dominant entry vector could have a number of forms. It is hard to parameterize it using simple parameters. In our simulations, we fix the length of D to be three and there is one distinguished large value in the vector. The vectors of dominant entries in conditional pdf are presented in Table II. They are the same for different j in $P(Y|X = j)$. Other than dominant entries, other entries have the same probability.

They are all $(3, 0.0015)$ -sparse conditional pdfs. Source X is uniformly distributed. For a vector of dominant entries, we define peak factor to be the ratio between the maximum entry and the minimum entry in the vector.

TABLE II
THE D VECTORS USED IN THE SIMULATIONS.

D	PF	D	PF
[0.15 0.6 0.15]	4	[0.1 0.6 0.1]	6
[0.1 0.7 0.1]	7	[0.1 0.75 0.1]	7.5
[0.1 0.79 0.1]	7.9	[0.05 0.6 0.05]	12
[0.05 0.7 0.05]	14	[0.03 0.6 0.03]	20

We show our simulation results in Fig. 2, in an ascending order of peak factor (PF). The plots do not look as smooth as Fig. 1. This is because peak factor is not a single parameter for the pdfs, e.g., for a fixed PF, there could be multiple choices of the pdf and we choose one of them in our simulation. The gaps between actual transmission rates and the conditional entropies are presented. The alphabet size $q = 256$. Both random form and diagonal form conditional pdf are investigated. For RS codes, the performance is the same under these two forms. We observe the following. The performance of RS codes improves with the increase of the PF. RS codes perform better than rate-adaptive LDPC codes under the correlation models with large PF, while rate-adaptive LDPC codes perform better than RS codes under the correlation models with small PF. However, dedicated LDPC codes outperform RS for most of PF values.

We also investigate the situation where the decoder is given a slightly different joint pdf. The actual pdf is in the diagonal form. The pdf provided to the decoder has right locations for the largest dominant entries but wrong (somewhat arbitrary) locations for another two smaller dominant entries in D . In this case, the performance of LDPC codes suffer a lot and RS codes suffer only a little. The results are also presented in Fig. 2. It is important to note that in this situation, RS codes in fact perform better than multistage LDPC codes. In a practical setting there may be situations where there are modeling errors or incomplete knowledge about the joint pdf of the sources. Our results indicate that RS codes are much more resilient to inaccuracies in correlation models.

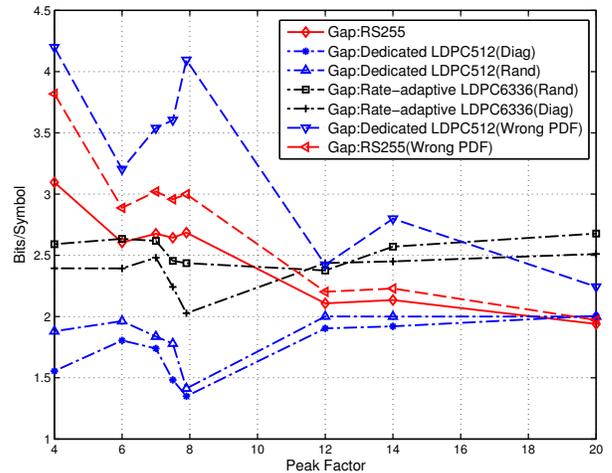


Fig. 2. The gap between the actual transmission rate and the conditional entropy for multistage LDPC codes and RS codes under sparse correlation models. For RS codes, the performance under diagonal form conditional distribution and random form conditional distribution are the same.

VI. COMPARISON WITH MULTISTAGE LDPC CODES: FEEDBACK SCENARIO

A. Simulation setting

We consider the second scenario where the decoder feeds back some information and the actual transmission rates are adapted such that the decoder is able to decode. RS codes offer natural rate-adaptivity and we compare their performance with the rate adaptive LDPC codes designed in [7]. For multistage LDPC codes, after receiving the binary syndromes from the encoder, the decoder tries to decode from the first bit source. If it fails, it requests more bits from the source and tries to decode again. The decoder repeats this procedure until the first bit source is decoded and then moves on to the second bit source and works in a similar manner. It is guaranteed that the previously decoded bits are always correct. Two rate-adaptive LDPC codes are used, with length 6336 and 396, both designed in [7]. For RS codes, if the decoder fails (there is no codeword on the candidate list), it requests more symbols from the source and tries again. The decoder repeats this until the source sequence is decoded. The amount of feedback is several bits per block for both LDPC codes and RS codes, depending on the gap. But LDPC codes need more feedback since the decoder needs to adjust rate for each bit source. We repeat this experiment 500 times and record the minimum required transmission rates. The simulation results are the average minimum required rates and their standard deviation.

B. q -ary symmetric correlation models

The gap of the average minimum transmission rate to the conditional entropy is presented in Fig. 1 (dash-dot lines). RS outperform rate-adaptive LDPC codes when the agreement probability is very high or very low. But for intermediate P_a , multistage LDPC codes perform better. For LDPC codes with length 6336, the standard deviations of the required rates are in the range of 0.08 and 0.1, while LDPC codes with length 396, the standard deviation are between 0.19 and 0.30. The standard deviations of RS codes are between 0.13 and 0.32.

C. Sparse correlation models

The gap of the average minimum transmission rate to $H(Y|X)$ is presented in Fig. 3. RS performs worse than both multistage LDPC codes, although the performance improves with the PF. The average rate performance is comparable between LDPC codes with length 6336 and 396, and between diagonal form and random form correlation models, but length 6336 codes are much more stable, with standard deviation 0.06 to 0.1. RS codes have standard deviation between 0.24 and 0.30, and length 396 LDPC codes have standard deviation between 0.11 and 0.27. The results for the case where inaccurate pdfs are provided to the decoder are also presented and we observe that RS codes are much more resilient and perform better than LDPC codes with length 6336.

VII. CONCLUSION

In this work we have proposed practical SW codes using RS codes. Compared to multistage LDPC codes, RS codes are easy to design, offer natural rate-adaptivity and allow for

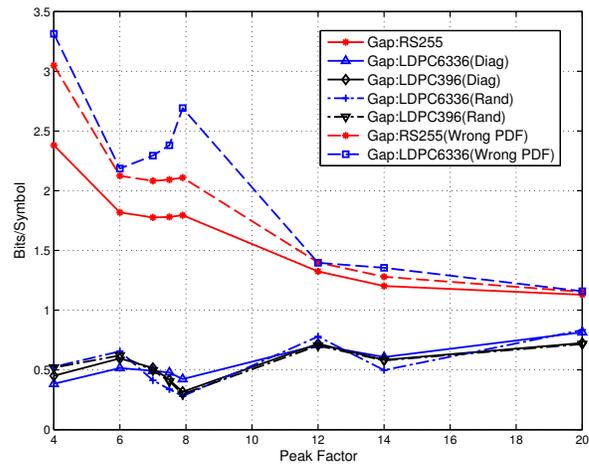


Fig. 3. The gap between the average minimum transmission rate and $H(Y|X)$ for multistage LDPC and RS codes under sparse correlation models.

relatively fast performance analysis. Simulations show that in classical SWC scenario, RS codes perform better than both designs of multistage LDPC codes under q -ary symmetric model and better than rate-adaptive LDPC codes under the sparse correlation model with high PF. In a feedback scenario, the performance of RS codes and multistage LDPC codes are similar under q -ary symmetric model but LDPC codes outperform RS codes under sparse correlation model. An interesting conclusion is that RS codes are much more resilient to inaccurate pdfs in both scenarios.

For symmetric Slepian-Wolf coding, if the correlation model is given by additive error, i.e., $X = Y + E$, it is not hard to propose a scheme that first recover the error vector e and then recover the source sequences. The more interesting and challenging problem is to apply algebraic approaches to more general correlation models, where the problem can not be mapped to a simple channel decoding problem. The problem remains open and will be an interesting future work.

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