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Abstract

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Keywords

multiuser MIMO, Power allocation, uplink, training, rate maximization

Disciplines

Electrical and Computer Engineering | Power and Energy | Signal Processing

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Joint Optimization of Power Allocation and Training Duration for Uplink Multiuser MIMO Communications

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Abstract—In this paper, we consider a multiuser multiple-input multiple-output (MU-MIMO) communication system between a base station equipped with multiple antennas and multiple mobile users each equipped with a single antenna. The uplink scenario is considered. The uplink channels are acquired by the base station through a training phase. Two linear processing schemes are considered, namely maximum-ratio combining (MRC) and zero-forcing (ZF). We optimize the training period and optimal training energy under the average and peak power constraint so that an achievable sum rate is maximized.

Index Terms—Power allocation, uplink, training, rate maximization, multiuser MIMO

I. INTRODUCTION

Multiuser Multiple-input multiple-output (MU-MIMO) systems are a type of cellular communication where the base station is equipped with multiple antennas. The base station serves multiple mobile stations that are usually equipped with a small number of antennas, typically one. MU-MIMO holds good potentials for improving future communication system performance. However, inter-cell interference or intra-cell interference decreases the achievable performance of adopting MU-MIMO such that complex techniques are involved inevitably. Therefore, there is a tradeoff of allocating the resources for MU-MIMO, such as the number of users which has been studied in [1], the training and feedback optimization in terms of training period and power is considered for downlink MIMO broadcast channel in [2].

Recently, massive MIMO technology has attracted much attention. In such a system, a large number of antennas at the base station are employed to improve the system performance. There is already a body of results in the literature about the analysis and design of large MIMO systems; see e.g., the overview article [3] and references therein. It is important to quantify the achievable performance of such systems in realistic scenarios. For example, channel state information (CSI) acquisition in uplink takes time, energy, and channel estimation error will always exist. For MU-MIMO, both circuit and transmission powers in uplink were considered when designing power allocation schemes [4], where energy efficiency is optimized.

In this paper, we are interested in performance of the uplink transmission in a single-cell system. In particular, we ask what rates can be achieved in the uplink by the mobile

users if we assume realistic channel estimation at the base station. The achievable rates of uplink MU-MIMO system with maximum-ratio combining (MRC) and zero-forcing (ZF) detection were derived in [5], and the performance evaluation was discussed in [6]. But the analysis therein assumes equal power transmission during the channel training phase and the data transmission phase, which is not optimal in the sense that sum rate is optimized. In previous study, the power allocation between training phase and data phase was investigated for MIMO case with optimizing effective signal-to-noise (SNR) in [7], which shows the tradeoff of energy splitting between the two phases such that the achievable rate can be maximized. However, the peak power was not considered before. If the training period is limited and the accurate estimate is required, then the peak power will be very high since we need to spend enough energy on training phase. In this case, the optimal power allocation strategy is not practical.

In this paper, the power allocation and training duration are both optimized for uplink MU-MIMO systems in a systematic way. Two linear receivers, MRC and ZF, are adopted with imperfect CSI. The average and peak power constraints are both incorporated. We analyze the convexity of this optimization problem, and derive the optimal solution. The solution is in closed form except in one case where a one-dimensional search of a quasi-concave function is needed. Simulation results are also provided to demonstrate the benefit of optimized training, compared to equal power allocation considered in the literature.

The main contribution of the work is that we provided a complete solution for the optimal training duration and training energy in an uplink MU-MIMO system with either MRC (or ZF) receiver, and with both peak and average power constraints.

II. MU MIMO SYSTEM MODEL

Consider an uplink MU-MIMO system. The base station is equipped with an array of M antennas. There are K mobile users, each with a single antenna. We assume $M > K$. For a massive MU-MIMO system, we have typically $M \gg K$.

A. Transmission Scheme

We assume that the channel follows a block fading model such that it remains constant during a block of T symbols,

and changes independently from block to block. The uplink transmission consists of two phases: training phase and data transmission phase. The training phase lasts for T_τ symbols, and the data phase lasts for $T_d = T - T_\tau$ symbols. We assume that the mobile users are synchronized.

1) *Training*: The training phase is used for the base station to acquire the CSI. During the training phase, the K users send time-orthogonal signals at power level ρ_τ per user. The training signals can be represented as a $K \times T_\tau$ matrix $\sqrt{T_\tau \rho_\tau} \mathbf{\Phi}$, where $\mathbf{\Phi}$ satisfies $\mathbf{\Phi} \mathbf{\Phi}^H = \mathbf{I}_K$. The received signal in training phase is

$$\mathbf{Y}_\tau = \sqrt{T_\tau \rho_\tau} \mathbf{H} \mathbf{\Phi} + \mathbf{N} \quad (1)$$

where \mathbf{H} denotes the fast fading channel matrix, whose entries are i.i.d. random variables which follow Gaussian distribution with zero mean and unit variance, i.e., $\mathcal{CN}(0, 1)$; \mathbf{N} is an $M \times T_\tau$ matrix with i.i.d. $\mathcal{CN}(0, 1)$ elements that represent the additive noise. The minimum mean-square error (MMSE) estimate

$$\hat{\mathbf{H}} = \frac{\sqrt{T_\tau \rho_\tau}}{T_\tau \rho_\tau + 1} \mathbf{Y}_\tau \mathbf{\Phi}^H \quad (2)$$

will be used for demodulating the data symbols during the data transmission phase. Note that we require $T_\tau \geq K$ to satisfy the time-orthogonality.

2) *Data Transmission*: In the data transmission phase, all users send signals with power ρ_d . The received signal is

$$\mathbf{y} = \sqrt{\rho_d} \mathbf{H} \mathbf{x} + \mathbf{n} \quad (3)$$

where \mathbf{x} is a $K \times 1$ vector denoting the transmitted symbols, and \mathbf{n} is a $M \times 1$ vector denoting the additive noise. We assume that the noise distribution is i.i.d. $\mathcal{CN}(0, 1)$.

B. Linear Receivers

Based on the model in (3), we will consider two linear demodulation schemes: MRC and ZF receivers. The demodulated symbols can be written as

$$\hat{\mathbf{x}} = \mathbf{G} \mathbf{y} \quad (4)$$

where \mathbf{G} is a $K \times M$ matrix that depends on the receiver type.

1) *MRC Receiver*: For MRC receiver, we have $\mathbf{G} = \hat{\mathbf{H}}^H$. The signal-to-interference plus noise ratio (SINR) for any of the K users' symbols can be obtained in the same way as in, e.g., [5, eq. (39)] as

$$\text{SINR}^{\text{MRC}} = \frac{T_\tau \rho_\tau \rho_d (M - 1)}{T_\tau \rho_\tau \rho_d (K - 1) + K \rho_d + T_\tau \rho_\tau + 1}. \quad (5)$$

2) *ZF Receiver*: For ZF receiver, $\mathbf{G} = \frac{1}{\sqrt{\rho_d}} (\hat{\mathbf{H}}^H \hat{\mathbf{H}})^{-1} \hat{\mathbf{H}}^H$. The expected value of SINR for any of the K users' symbols can be obtained in the same way as in, e.g., [5, eq. (42)] as

$$\text{SINR}^{\text{ZF}} = \frac{T_\tau \rho_\tau \rho_d (M - K)}{K \rho_d + T_\tau \rho_\tau + 1}. \quad (6)$$

For either receiver, a lower bound on the sum rate achieved by the K users is given by

$$R^A(\alpha, T_d) = \frac{T_d}{T} K \log_2(1 + \text{SINR}^A) \quad (7)$$

where $A \in \{\text{MRC}, \text{ZF}\}$.

C. Power Allocation

We assume that the transmitters are subject to both peak and average power constraints.

1) *Average Power Constraint*: We assume the average transmitted power over one coherence interval T is equal to a given constant ρ , namely $\rho_d T_d + \rho_\tau T_\tau = \rho T$. Let $\alpha := \rho_\tau T_\tau / (\rho T)$ denote the fraction of the total transmit energy that is devoted to channel training; i.e.,

$$\rho_\tau T_\tau = \alpha \rho T, \quad \rho_d T_d = (1 - \alpha) \rho T, \quad 0 \leq \alpha \leq 1. \quad (8)$$

2) *Peak Power Constraint*: The peak power during the transmission is assumed to be no more than ρ_{\max} ; i.e.,

$$0 \leq \rho_d, \rho_\tau \leq \rho_{\max}. \quad (9)$$

D. Optimization Problem

For an adopted receiver, $A \in \{\text{MRC}, \text{ZF}\}$, our goal is to maximize the uplink achievable rate subject to the peak and average power constraints. That is,

$$\underset{\alpha, T_d}{\text{maximize}} \quad R^A(\alpha, T_d) \quad (10)$$

$$\text{subject to} \quad T_d + T_\tau = T \quad (11)$$

$$\rho T \alpha + \rho_{\max} T_d \leq \rho_{\max} T \quad (12)$$

$$-\rho T \alpha - \rho_{\max} T_d \leq -\rho T \quad (13)$$

$$0 \leq \alpha \leq 1 \quad (14)$$

$$0 < T_d \leq T - K \quad (15)$$

where $R^A(\alpha, T_d)$ is as given in (7); (12) and (13) are from the peak power constraints in the training and data phases, respectively; and the last constraint is from the requirement that $T_\tau \geq K$.

III. SINR MAXIMIZATION WITH α FOR FIXED T_d

The feasible set of the optimization problem (10)–(15) is convex, but the convexity of the objective function is not obvious. In this section, we consider the optimization problem when T_d is fixed. In this case, we will prove that $R^A(\alpha, T_d)$ is concave in α , and derive the optimized α . The result will be useful in the next section that α and T_d are jointly optimized.

For a fixed T_d , from the peak power constraints (12) and (13), we have

$$\frac{\rho_{\max} T_\tau}{\rho T} + \left(1 - \frac{\rho_{\max}}{\rho}\right) \leq \alpha \leq \frac{\rho_{\max} T_\tau}{\rho T}. \quad (16)$$

Combined with (14), the overall constraints on α is

$$\min\left\{0, \frac{\rho_{\max} T_\tau}{\rho T} + \left(1 - \frac{\rho_{\max}}{\rho}\right)\right\} \leq \alpha \leq \max\left\{\frac{\rho_{\max} T_\tau}{\rho T}, 1\right\}. \quad (17)$$

In the remaining part of this section, we will first ignore the peak power constraint, and derive the optimal $\alpha \in (0, 1)$ for a given T_d . At the end of this section, we will reconsider the effect of the peak power constraint on the optimal α .

A. MRC Case without peak power constraint

Using (8) we can rewrite (5) as

$$\text{SINR}^{\text{MRC}}(\alpha) = \frac{M-1}{K-1} \frac{\alpha(\alpha-1)}{\alpha^2 - a_1\alpha - b_1} \quad (18)$$

where

$$a_1 = 1 + \frac{T_d - K}{\rho T(K-1)}, \quad b_1 = \frac{\rho T K + T_d}{\rho^2 T^2 (K-1)} > 0. \quad (19)$$

It can be verified that $1 - a_1 - b_1 \leq 0$.

1) *Behavior of the SINR^{MRC}(α) function:* Define

$$g(\alpha) := \text{SINR}^{\text{MRC}} \cdot (K-1)/(M-1). \quad (20)$$

And let $g_d(\alpha) = \alpha^2 - a_1\alpha - b_1$, which is the denominator of $g(\alpha)$.

Remark 1: It can be observed that when $1 - a_1 - b_1 \leq 0$ and $b_1 > 0$, $g_d(\alpha)$ is negative at both $\alpha = 0$ and $\alpha = 1$. Since the leading coefficient of $g_d(\alpha)$ is positive, $g_d(\alpha) < 0$ for $\alpha \in (0, 1)$, and it has no root in $(0, 1)$.

Lemma 1: The function $g(\alpha)$ is concave in α over $(0, 1)$ when $1 - a_1 - b_1 \leq 0$ and $b_1 > 0$.

Proof: See Appendix A. ■

According to Lemma 1, we know that there is a global maximal point for (18). Take the derivative of (18) and set it as 0, we have

$$(1 - a_1)\alpha^2 - 2b_1\alpha + b_1 = 0. \quad (21)$$

Based on Remark 1, we deduce that $g(\alpha) > 0$ for $\alpha \in (0, 1)$. In addition, we have $g(0) = 0$ and $g(1) = 0$. Therefore, there is an optimal α within $(0, 1)$ rather than at boundaries.

2) *The optimizing α :* We discuss the optimal α in three cases, depending on T_d , as compared to K .

1) If $T_d = K$, then $1 - a_1 = 0$. Hence, we have $\alpha^* = 1/2$, and

$$\text{SINR}^{\text{MRC}}\left(\frac{1}{2}\right) = \frac{M-1}{K-1} \frac{1/4}{1/4 + \frac{K(\rho T + 1)}{\rho^2 T^2 (K-1)}} \quad (22)$$

2) If $T_d < K$, then $1 - a_1 > 0$. Since $b_1 > 1 - a_1$, $b_1/(1 - a_1) > 1$. Between the two roots of (21), the one in between 0 and 1 is

$$\alpha^* = \frac{b_1 - \sqrt{b_1(a_1 + b_1 - 1)}}{1 - a_1}. \quad (23)$$

3) If $T_d > K$, then $1 - a_1 < 0$. It can be deduced that in this case α^* in (23) is still between 0 and 1 and therefore is the optimal α .

Substituting (19) into (23), we have

$$\alpha^* = \frac{\sqrt{(\rho T K + T_d)(\rho T T_d + T_d)} - (\rho T K + T_d)}{\rho T (T_d - K)}. \quad (24)$$

We can simplify the expression for the optimal α at high and low SNR:

1) At high SNR, the optimal α^* is

$$\alpha^*_H \approx \frac{\sqrt{K T_d} - K}{T_d - K}. \quad (25)$$

2) Similarly, at low SNR, the optimal α^* is

$$\alpha^*_L \approx \frac{1}{2}. \quad (26)$$

As a result, $\text{SINR}^{\text{MRC}}(\alpha^*_L) = (M-1)/(4T_d(K-1))$. If the SNR is low, the fraction between the training and data is independent on the system parameters M , K , ρ_d , ρ_τ , T_τ , and T .

B. ZF Case without peak power constraint

This optimization problem in the ZF case is similar to that in [7, eq. 22], which maximizes the effective SNR for MIMO system with MMSE receiver. Here, we only give the final optimization results.

1) *The SINR function:* Using (8) we can rewrite (6) as

$$\text{SINR}^{\text{ZF}}(\alpha) = \frac{T\rho(M-K)\alpha(1-\alpha)}{(T_d-K)(\gamma+\alpha)} \quad (27)$$

where $\gamma = \frac{K\rho T + T_d}{\rho T(T_d - K)}$. The second derivative of (27) is

$$-2T\rho(M-K)\gamma(\gamma+1)/[(T_d-K)(\alpha+\gamma)^3], \quad (28)$$

which we will consider to decide the convexity of the objective function. It can be verified that in all the three cases, namely $T_d = K$, $T_d > K$, and $T_d < K$, $\text{SINR}^{\text{ZF}}(\alpha)$ is concave in α within $\alpha \in (0, 1)$.

2) *The optimizing α^* :* Taking the first derivative of (27) and set to 0, we can obtain the optimal α^* :

- 1) When $T_d = K$, $\alpha^* = 1/2$.
- 2) When $T_d > K$, $\alpha^* = -\gamma + \sqrt{\gamma(\gamma+1)}$.
- 3) When $T_d < K$, $\alpha^* = -\gamma - \sqrt{\gamma(\gamma+1)}$.

We can simplify the expression for the optimal α at high and low SNR:

- 1) At high SNR, $\gamma = K/(T_d - K)$.
- 2) At low SNR, $\gamma = T_d/(\rho T(T_d - K))$, $\alpha^*_L = 1/2$ which is consistent with the MRC case.

C. MRC and ZF with peak power constraint

So far we have ignored the peak power constraint. When the peak power is considered, and α^* is not within the feasible set (17), the optimal $\tilde{\alpha}^*$ with the peak power constraint is the α within the feasible set that is closest to the α^* we derived, which is at one of the two boundaries of the feasible set, due to the concavity of the objective function.

IV. ACHIEVABLE RATE MAXIMIZATION WITH α AND T_d

In this section, α and T_d are jointly optimized for maximizing the achievable rate of uplink MU-MIMO system as illustrated in (10)–(15) when both average and peak power constraints are considered.

The feasible set with respect to α and T_d is illustrated in Fig. 1. It can be observed that the feasible region is in between the following two lines

$$T_d = -\rho T \alpha / \rho_{\max} + T, \quad (29)$$

$$T_d = -\rho T \alpha / \rho_{\max} + \rho T / \rho_{\max} \quad (30)$$

where α and T_d satisfy (14) and (15).

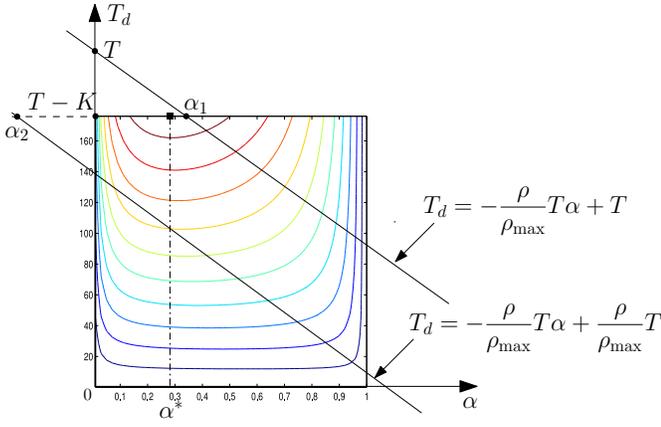


Fig. 1. Feasible region and the contour of the objective function in the MRC case; $T = 196$, $K = 20$ and $M = 50$.

We have the following lemma that is useful for describing the behavior of our objective function $\text{SINR}^A(\alpha, T_d)$ when α is fixed.

Lemma 2: The function $f(x) = x \ln(1 + a/(b + cx))$, when $a, b, c, x > 0$, is concave and monotonically increasing.

Proof: See Appendix B. ■

In summary, the convexities of the objective function are known to have the following two properties:

- (P1) From Lemma 1, for fixed T_d , R^A is a concave function with respect to α .
- (P2) From Lemma 2, for fixed α , R^A is a concave function and monotonically increasing with respect to T_d .

Since the feasible set is convex, our optimization problem (10)–(15) is a biconvex problem that may include multiple local optimal solutions. However, after studying the convexities of the objective function, there are only three possible cases for the optimal solutions, as we discuss below.

In the remainder of this section, let α^\dagger denote the optimal α when $T_d = T - K$.

A. Case 1: ρ_τ is limited by ρ_{\max}

Define $\alpha_1 := \rho_{\max}K/\rho T$, which is the root of $T - K = -\rho T\alpha/\rho_{\max} + T$ in α ; see Figure 1. In the case where $\alpha_1 < \alpha^\dagger$, because of the property P2 the optimal (α^*, T_d^*) must be on one of the two lines given by i) $T_d = -\rho T\alpha/\rho_{\max} + T$, $\alpha \in [\alpha_1, 1]$, and ii) $T_d = T - K$, $\alpha \in [0, \alpha_1]$.

On the line $T_d = T - K$, $\alpha \in [0, \alpha_1]$ the objective function is concave and increasing with α , thanks to property P1. Hence, we only need to consider the line $T_d = -\rho T\alpha/\rho_{\max} + T$, $\alpha \in [\alpha_1, 1]$.

Lemma 3: The objective function $R^{\text{MRC}}(\alpha, T_d)$ along the line $T_d = -\rho T\alpha/\rho_{\max} + T$, $\alpha \in [\alpha_1, 1]$ is quasiconcave in α .

Proof: Consider MRC processing. Substituting (29) into $R^{\text{MRC}}(\alpha, T_d)$, we have

$$R^{\text{MRC}}(\alpha) = \frac{K}{T} \left(-\frac{\rho T}{\rho_{\max}} \alpha + T \right) \log_2(1 + \text{SINR}^{\text{MRC}}) \quad (31)$$

where

$$\text{SINR}^{\text{MRC}}(\alpha) = \frac{\alpha(\alpha - 1)\rho^2 T^2(M - 1)}{a_2 \alpha^2 - b_2 \alpha - c_2}, \quad (32)$$

and $a_2 = \rho^2 T^2(K - 1) + \rho^2 T^2/\rho_{\max}$, $b_2 = \rho^2 T^2(K - 1) + \rho T^2 - \rho T K - \rho T\alpha/\rho_{\max}$ and $c_2 = K\rho T + T$. Since $R^{\text{MRC}}(\alpha) > 0$, in order to prove the quasi-concavity of $R^{\text{MRC}}(\alpha)$, we need to prove that the super-level set $\mathcal{S}_\beta = \{\alpha | 0 < \alpha < 1, R^{\text{MRC}}(\alpha) \geq \beta\}$ for each $\beta \in \mathbb{R}^+$ is convex. Equivalently, if we define

$$\phi_\beta(\alpha) = \frac{\beta}{\frac{K}{T} \left(\frac{\rho T \alpha}{\rho_{\max}} - T \right)} + \log_2(1 + \text{SINR}^{\text{MRC}}(\alpha)). \quad (33)$$

we only need to prove that $\mathcal{S}_\phi = \{\alpha | 0 < \alpha < 1, \phi_\beta(\alpha) \geq 0\}$ is a convex set.

It can be checked that the first part of $\phi_\beta(\alpha)$, namely $\beta / [\frac{K}{T} (\frac{\rho T \alpha}{\rho_{\max}} - T)]$, is concave for $\alpha \in [0, 1]$. For the other part of $\phi_\beta(\alpha)$, from (32) we know that

$$a_2 - b_2 - c_2 = \rho T \left(\frac{\rho}{\rho_{\max}} - 1 \right) - T \left(1 - \alpha \frac{\rho}{\rho_{\max}} \right) < 0 \quad (34)$$

where $a_2, c_2 > 0$. Applying Lemma 1, we know $\text{SINR}^{\text{MRC}}(\alpha)$ is concave. Hence, $\log_2(1 + \text{SINR}^{\text{MRC}}(\alpha))$ is also concave since function $\log(1 + x)$ is concave and nondecreasing [8]. Therefore, its super-level set \mathcal{S}_ϕ is convex. It follows that the super-level set \mathcal{S}_β of $R^{\text{MRC}}(\alpha)$ is convex for each $\beta \geq 0$. The objective function is thus quasiconcave. ■

Thanks to Lemma 3, we can find the optimal α by setting the derivative of (31) with respect to α to 0. Efficient one-dimensional searching algorithm such as Newton method or bisection algorithm [8], can be adopted to find out the optimal α .

B. Case 2: ρ_d is limited by ρ_{\max}

Define $\alpha_2 := 1 - \rho_{\max}(T - K)/\rho T$, which is the root of $T - K = \rho T\alpha/\rho_{\max} + \rho T/\rho_{\max}$ in α . If $\alpha_2 > \alpha^\dagger$, because of the property P2 the optimal (α^*, T_d^*) must be on one of the two lines given by i) $T_d = -\rho T\alpha/\rho_{\max} + T$, $\alpha \in (\alpha_1, 1)$, $\alpha \in [\alpha_1, 1]$, and ii) $T_d = T - K$, $\alpha \in [\alpha_2, \alpha_1]$. Along the line $T_d = T - K$, $\alpha \in (\alpha_1, 1)$, the corresponding function is decreasing in α because of the property P1. Also considering P2, which implies that the optimal point in this case cannot include $T_d < T - K$, we conclude that the point $(\alpha^*, T_d^*) = (\alpha_2, T - K)$ is the global optimal solution of the problem.

C. Case 3: Neither ρ_d nor ρ_τ is not limited by ρ_{\max}

If $\alpha_2 < \alpha^\dagger < \alpha_1$, the optimal point is achieved at $(\alpha^*, T_d^*) = (\alpha^\dagger, T - K)$, according to properties P1 and P2.

Summarizing what we have discussed so far, we have the following theorem.

Theorem 1: For the MRC receiver, set $\alpha^\dagger = 1/2$ if $T_d = K$ and otherwise set α^\dagger according to (24) when $T_d = T - K$. Set $\alpha_1 = \rho_{\max}K/\rho T$ and set $\alpha_2 = 1 - \rho_{\max}(T - K)/\rho T$. There are three cases: Case 1) If $\alpha_1 < \alpha^\dagger$, then α^* is given by the maximizer of $R^{\text{MRC}}(\alpha)$ in (31), and $T_d^* = -\rho T\alpha^*/\rho_{\max} + T$; Case 2) If $\alpha_2 > \alpha^\dagger$ then $(\alpha^*, T_d^*) = (\alpha_2, T - K)$; Case 3) If $\alpha_2 < \alpha^\dagger < \alpha_1$, then $(\alpha^*, T_d^*) = (\alpha^\dagger, T - K)$.

We also have similar results regarding the optimal energy allocation factor α and training period T_r for the ZF case. Due to the space limit, the result is not included here.

We also remark that our results are applicable for any $M > K$. When $M \gg K$, the system is known as a “massive MIMO” system. Our results offer optimal training energy allocation and optimal training duration when there is a peak power constraint in addition to the average power constraint.

V. NUMERICAL RESULTS

In this section, we compare the achievable rates between equal power allocation scheme and our optimized one under average and peak power constraints. In our simulations, we set $\rho_{\max} = 1.2\rho$, $K = 10$, and $T = 196$. We consider the following schemes: 1) MRC, which refers to the case where MRC receiver is used and the same average power is used in both training and data transmission phases [5]. 2) optimized MRC, which refers to the case where MRC receiver is used, the training duration is K , and there is no peak power constraint. 3) power-limited MRC, where MRC receiver is used, and both the training duration and training energy are optimized under both the average and peak power constraints. We will also consider the ZF variants of the above three cases, namely ZF, optimized ZF, and power-limited ZF. The energy efficiency is defined as $\eta^A := R^A(\alpha, T_d)/\rho$.

In Fig. 2, we show the achieved rates of various schemes as the number of antennas increases. It can be seen that the optimized MRC (ZF) performs better than the unoptimized MRC (ZF) as well as the peak-power limited MRC (ZF). In Fig. 3, the energy efficiency is shown as a function of ρ . It can be seen that there is an optimal average transmitted power for maximal energy efficiency. It can also be seen that optimized schemes show a significant gain when ρ is small, since the power resource is precious. In Fig. 4, we show the energy efficiency versus sum rate. It can be observed that the energy efficiency is maximized at a certain rate. In particular, the optimized schemes achieve higher energy efficiencies. Also from the simulations, we can see that ZF performs better than MRC at high SNR, but worse when SNR is low.

VI. CONCLUSION

In this paper, we considered a uplink MU-MIMO system with training and data transmission phases. Two receivers were considered, namely MRC and ZF receivers. Power allocation between training phase and data phase, and the training duration were optimized such that an achievable rate was maximized. Both average and peak power constraints were considered. We performed a careful analysis of the convexity of the problem and derived optimal solution either in closed form or in one case through a one-dimensional search for a quasi-concave function. Our results were illustrated through numerical examples, for some example system setups including those with a large number of antennas at the base station.

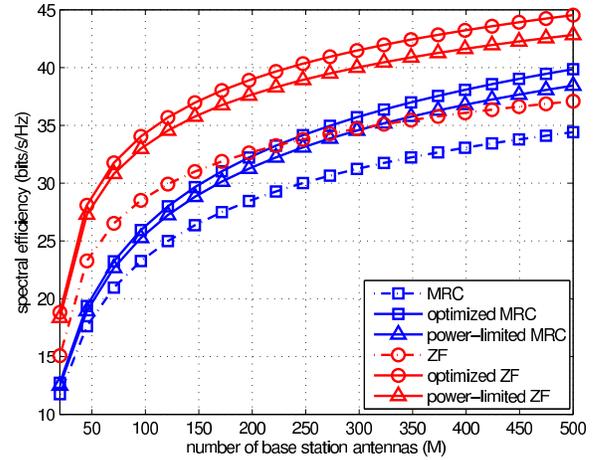


Fig. 2. Comparison between equally power allocation and the optimized fraction α in terms of the number of base station antennas, where $\rho = -5\text{dB}$.

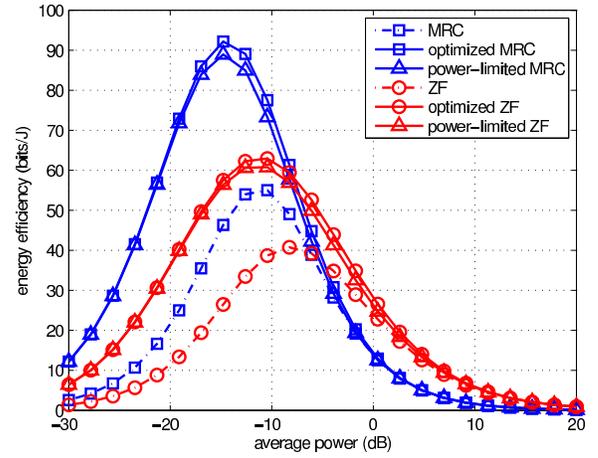


Fig. 3. Comparison of energy efficiency in terms of the transmitted power ρ , where $M = 20$.

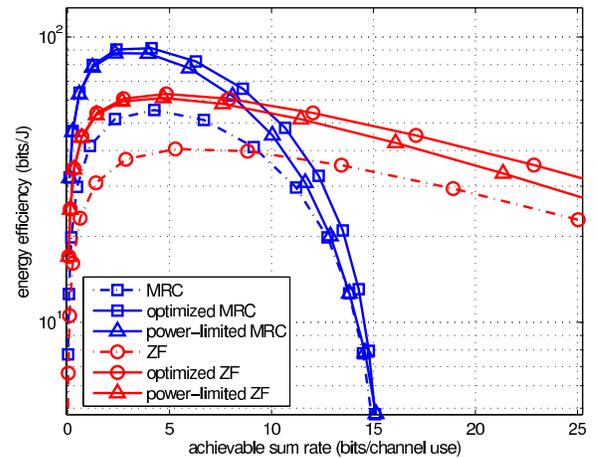


Fig. 4. Comparison of energy efficiency versus the spectral efficiency, where $M = 20$.

VII. APPENDIX

A. Proof of Lemma 1

Replacing α as x in (18), we need to verify that the second derivative of (18) with respect to x is negative [8]. The first derivative of $g(x)$ is

$$g'(x) = \frac{(1-a)x^2 - 2bx + b}{(x^2 - ax - b)^2} \quad (35)$$

where $1 - a - b < 0$, $b > 0$ and $x \in (0, 1)$. Then, take the second derivative of $g(x)$, we have

$$g''(x) = \frac{2}{(x^2 - ax - b)^3} \underbrace{((a-1)x^3 + 3bx^2 - 3bx + ab + b^2)}_{f(x)} \quad (36)$$

From Remark 1 and $b > 0$, we know that $(x^2 - ax - b)^3 < 0$. The goal of the proof becomes to show $f(x) > 0$.

Checking the boundary of $f(x)$, we know that

$$f(0) = ab + b^2 = b(b+a) > b > 0, \quad (37)$$

$$f(1) = ab + b^2 = a - 1 + ab + b^2 = (a+b-1)(b+1) > 0. \quad (38)$$

Next, we need to consider the monotonicity of the function during the interval $x \in (0, 1)$. Take the derivative of $f(x)$, we get

$$\begin{aligned} f'(x) &= 3(a-1)x^2 + 6bx - 3b \\ &= 3(a-1)\left(x^2 + \frac{2b}{a-1}x - \frac{b}{a-1}\right), \end{aligned} \quad (39)$$

which is a quadratic function.

When $a = 1$, $f'(x) = 6bx - 3b = 3b(2x - 1)$. The function is decreasing until $x = 1/2$ and increasing afterwards. Since

$$f\left(\frac{1}{2}\right) = \frac{1}{4}b + b^2 > 0, \quad (40)$$

it can be deduced that $f(x) > 0$.

When $a \neq 1$, we know that $f'(1) = 3(a+b-1) > 0$, $f'(0) = -3b$, meaning that the function $f(x)$ is decreasing first and increasing after the minimum point.

Here, we need to verify the minimum value of $f(x^*)$ is always greater than 0. According to (39), the minimum point given by the root of $f'(x^*) = 0$ is

$$x^* = -\frac{b}{a-1} + \sqrt{\frac{b(a+b-1)}{(a-1)^2}}, \quad (41)$$

since $a+b > 1$ and $b > 0$. Substituting (41) into $f(x)$, we have

$$\begin{aligned} f(x) &= x((a-1)x^2 + 2bx - b) + bx^2 - 2bx + ab + b^2 \\ &\stackrel{(a)}{=} bx^2 + \frac{2b^2}{a-1}x - \frac{b^2}{a-1} - \frac{2b^2}{a-1}x + \frac{b^2}{a-1} \\ &\quad - 2bx + ab + b^2 \\ &\stackrel{(a)}{=} -\frac{2b(b+a-1)}{a-1}x + \frac{ab(a+b-1)}{a-1} \\ &= \frac{b(a+b-1)}{a-1} \underbrace{\left(\frac{2b}{a-1} - 2\sqrt{\frac{b(a+b-1)}{(a-1)^2}} + a\right)}_{h(x)} \end{aligned} \quad (42)$$

where (a) is according to $f'(x^*) = 0$.

For $a-1 > 0$,

$$\begin{aligned} h(x) &= \frac{2b}{a-1} - \frac{\sqrt{b(a+b-1)}}{a-1} + a \\ &= \frac{2}{a-1} \frac{b^2 - b(a+b-1)}{b + \sqrt{b(a+b-1)}} + a \end{aligned} \quad (43)$$

$$\stackrel{(b)}{>} a - \frac{2b}{b + \sqrt{b^2}} > 0 \quad (44)$$

where (b) is based on $a-1 > 0$. Therefore, $f(x) > 0$.

For $a-1 < 0$,

$$h(x) = \frac{2b}{a-1} + \frac{2\sqrt{b(a+b-1)}}{a-1} + a \quad (45)$$

$$\stackrel{(c)}{<} \frac{2(1-a)}{a-1} + a < 0, \quad (46)$$

where (c) is due to $b > 1 - a$. Hence, $f(x) > 0$.

B. Proof of Lemma 2

The derivative of $f(x) = x \ln(1 + a/(b+cx))$, where $a, b, c, x > 0$, is

$$f'(x) = \ln\left(1 + \frac{a}{cx+b}\right) - \frac{acx}{(cx+a+b)(cx+b)} \quad (47)$$

It is clear that $\lim_{x \rightarrow \infty} f'(x) = 0$. If we can verify that the function $f'(x)$ is monotonically decreasing, then $f'(x)$ is always positive. Hence, we take the second derivative of $f'(x)$, and get

$$f''(x) = -\frac{abc^2x + ac^2(a+b)x + 2ac(a+b)b}{[(cx+b)(cx+a+b)]^2} < 0, \quad (48)$$

since $a, b, c, x > 0$. This means that $f'(x)$ is decreasing. Therefore, $f'(x)$ is always positive, i.e., $f(x)$ is an increasing and concave function.

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